

16-BIT, 1-MSPS, PSEUDO-BIPOLAR, UNIPOLAR INPUT, MICROPOWER SAMPLING ANALOG-TO-DIGITAL CONVERTER WITH PARALLEL INTERFACE AND REFERENCE

FEATURES

- 0 to 1 MSPS Sampling Rate
- ± 0.7 LSB Typ, ± 1 LSB Max INL
- ± 0.4 LSB Typ, ± 0.75 LSB Max DNL
- 16-Bit NMC Ensured Over Temperature
- ± 0.1 mV Offset Error
- ± 0.15 ppm/ $^{\circ}$ C Offset Error Drift
- ± 0.015 %FSR Gain Error
- ± 0.7 ppm/ $^{\circ}$ C Gain Error Drift
- 93 dB SNR, -110dB THD, 112dB SFDR
- Zero Latency
- Low Power: 220 mW at 1 MSPS
- Unipolar Input Range: 0 V to V_{ref}
- Onboard Reference
- Onboard Reference Buffer
- High-Speed Parallel Interface
- Wide Digital Supply 2.7 V ~ 5.25 V
- 8-/16-Bit Bus Transfer

- 48-Pin 7x7 QFN Package

APPLICATIONS

- Medical Instruments
- Optical Networking
- Transducer Interface
- High Accuracy Data Acquisition Systems
- Magnetometers

DESCRIPTION

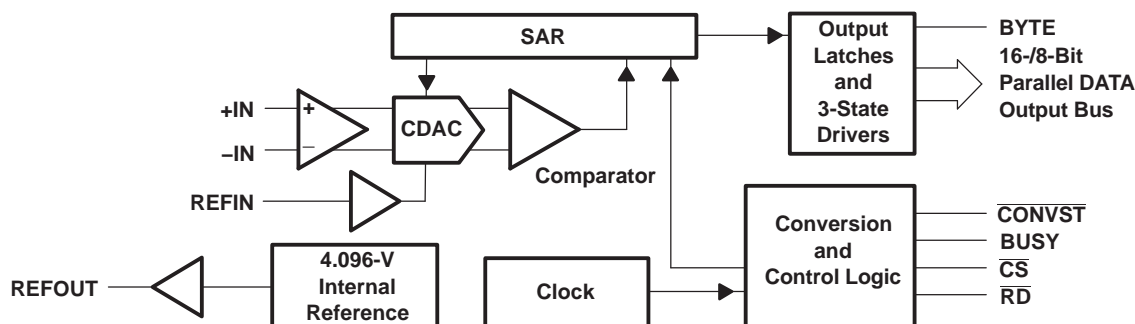
The ADS8471 is a 16-bit, 1-MSPS A/D converter with an internal 4.096-V reference and a pseudo-bipolar, unipolar input. The device includes a 16-bit capacitor-based SAR A/D converter with inherent sample and hold. The ADS8471 offers a full 16-bit interface or an 8-bit bus option using two read cycles.

The ADS8471 is available in a 48-lead 7x7 QFN package and is characterized over the industrial -40° C to 85° C temperature range.

HIGH-SPEED SAR CONVERTER FAMILY⁽¹⁾

TYPE/SPEED	500 kHz	580 kHz	750 kHz	1 MHz	1.25 MHz	2 MHz	3 MHz	4MHz
18-Bit Pseudo-Diff	ADS8383	ADS8381						
		ADS8380 (S)						
18-Bit Pseudo-Bipolar, Fully Diff		ADS8382 (S)		ADS8482	ADS8484			
16-Bit Pseudo-Diff	ADS8327 (S)	ADS8370 (S)	ADS8371	ADS8471	ADS8401	ADS8411		
	ADS8328 (S)			ADS8329/30 (S)	ADS8405	ADS8410 (S)		
16-Bit Pseudo-Bipolar, Fully Diff		ADS8372 (S)		ADS8472	ADS8402	ADS8412		ADS8422
					ADS8406	ADS8413 (S)		
14-Bit Pseudo-Diff					ADS7890 (S)		ADS7891	
12-Bit Pseudo-Diff				ADS7886				ADS7881

(1) S: Serial



Please be aware that an important notice concerning availability, standard warranty, and use in critical applications of Texas Instruments semiconductor products and disclaimers thereto appears at the end of this data sheet.



These devices have limited built-in ESD protection. The leads should be shorted together or the device placed in conductive foam during storage or handling to prevent electrostatic damage to the MOS gates.

ORDERING INFORMATION⁽¹⁾

MODEL	MAXIMUM INTEGRAL LINEARITY (LSB)	MAXIMUM DIFFERENTIAL LINEARITY (LSB)	NO MISSING CODES RESOLUTION (BIT)	PACKAGE TYPE	PACKAGE DESIGNATOR	TEMPERATURE RANGE	ORDERING INFORMATION	TRANSPORT MEDIA QTY.
ADS8471I	±2	±1	16	7x7 48 Pin QFN	RGZ	-40°C to 85°C	ADS8471IRGZT	Tape and reel 250
							ADS8471IRGZR	Tape and reel 1000
ADS8471IB	±1	±0.75	16	7x7 48 Pin QFN	RGZ	-40°C to 85°C	ADS8471IBRGZT	Tape and reel 250
							ADS8471IBRGZR	Tape and reel 1000

(1) For the most current package and ordering information, see the Package Option Addendum at the end of this document, or see the TI website at www.ti.com.

ABSOLUTE MAXIMUM RATINGS⁽¹⁾

over operating free-air temperature range (unless otherwise noted)

		VALUE	UNIT
Voltage	+IN to AGND	-0.4 to +VA + 0.1	V
	-IN to AGND	-0.4 to 0.5	V
	+VA to AGND	-0.3 to 7	V
	+VBD to BDGND	-0.3 to 7	V
	+VA to +VBD	-0.3 to 2.55	V
Digital input voltage to BDGND		-0.3 to +VBD + 0.3	V
Digital output voltage to BDGND		-0.3 to +VBD + 0.3	V
T _A	Operating free-air temperature range	-40 to 85	°C
T _{stg}	Storage temperature range	-65 to 150	°C
Junction temperature (T _J max)		150	°C
QFN package	Power dissipation	(T _J Max - T _A)/θ _{JA}	
	θ _{JA} thermal impedance	22	°C/W
Lead temperature, soldering	Vapor phase (60 sec)	215	°C
	Infrared (15 sec)	220	°C

(1) Stresses beyond those listed under *absolute maximum ratings* may cause permanent damage to the device. These are stress ratings only, and functional operation of the device at these or any other conditions beyond those indicated under *recommended operating conditions* is not implied. Exposure to absolute-maximum-rated conditions for extended periods may affect device reliability.

SPECIFICATIONS
 $T_A = -40^{\circ}\text{C}$ to 85°C , $+V_A = 5\text{ V}$, $+V_{BD} = 3\text{ V}$ or 5 V , $V_{\text{ref}} = 4.096\text{ V}$, $f_{\text{SAMPLE}} = 1\text{ MSPS}$ (unless otherwise noted)

PARAMETER		TEST CONDITIONS	MIN	TYP	MAX	UNIT	
ANALOG INPUT							
Full-scale input voltage ⁽¹⁾		+IN – (–IN)	0		V_{ref}	V	
Absolute input voltage		+IN	–0.2		$V_{\text{ref}} + 0.2$	V	
		–IN	–0.2		0.2		
Input capacitance				65		pF	
Input leakage current				1		nA	
SYSTEM PERFORMANCE							
Resolution				16		Bits	
No missing codes		ADS8471I		16		Bits	
		ADS8471IB		16			
INL	Integral linearity ⁽²⁾ ⁽³⁾	ADS8471I	–2	± 0.7	2	LSB (16 bit)	
		ADS8471IB	–1	± 0.7	1		
DNL	Differential linearity	ADS8471I	–1	± 0.4	1	LSB (16 bit)	
		ADS8471IB	–0.75	± 0.4	0.75		
Offset error ⁽⁴⁾		ADS8471I	–0.5	± 0.1	0.5	mV	
		ADS8471IB	–0.5	± 0.1	0.5		
Offset error temperature drift		ADS8471I		± 0.15		ppm/ $^{\circ}\text{C}$	
		ADS8471IB		± 0.15			
Gain error ⁽⁴⁾ ⁽⁵⁾		ADS8471I	$V_{\text{ref}} = 4.096\text{ V}$	–0.075	± 0.015	0.075	%FS
		ADS8471IB	$V_{\text{ref}} = 4.096\text{ V}$	–0.075	± 0.015	0.075	%FS
Gain error temperature drift		ADS8471I		± 0.7		ppm/ $^{\circ}\text{C}$	
		ADS8471IB		± 0.7			
Noise				25		μV RMS	
Power supply rejection ratio		At FFFFh output code		60		dB	
SAMPLING DYNAMICS							
Conversion time				670	700	ns	
Acquisition time			270	300		ns	
Throughput rate					1	MHz	
Aperture delay				4		ns	
Aperture jitter				5		ps	
Step response				150		ns	
Overvoltage recovery				150		ns	

- (1) Ideal input span, does not include gain or offset error.
- (2) LSB means least significant bit
- (3) This is endpoint INL, not best fit.
- (4) Measured relative to an ideal full-scale input [+IN – (–IN)] of 8.192 V
- (5) This specification does not include the internal reference voltage error and drift.

SPECIFICATIONS (Continued)

$T_A = -40^{\circ}\text{C}$ to 85°C , $+V_A = 5\text{ V}$, $+V_{BD} = 3\text{ V}$ or 5 V , $V_{ref} = 4.096\text{ V}$, $f_{SAMPLE} = 1\text{ MSPS}$ (unless otherwise noted)

PARAMETER		TEST CONDITIONS	MIN	TYP	MAX	UNIT
DYNAMIC CHARACTERISTICS						
THD	Total harmonic distortion ⁽¹⁾	ADS8471I	$V_{IN} = 4 V_{pp}$ at 2 kHz	-110	dB	
		ADS8471IB		-112		
		ADS8471I	$V_{IN} = 4 V_{pp}$ at 20 kHz	-105		
		ADS8471IB		-107		
		ADS8471I	$V_{IN} = 4 V_{pp}$ at 100 kHz	-101		
		ADS8471IB		-102		
SNR	Signal-to-noise ratio ⁽¹⁾	ADS8471I	$V_{IN} = 4 V_{pp}$ at 2 kHz	93	dB	
		ADS8471IB		93		
		ADS8471I	$V_{IN} = 4 V_{pp}$ at 20 kHz	92.5		
		ADS8471IB		92.7		
		ADS8471I	$V_{IN} = 4 V_{pp}$ at 100 kHz	91.5		
		ADS8471IB		91.6		
SINAD	Signal-to-noise + distortion ⁽¹⁾	ADS8471I	$V_{IN} = 4 V_{pp}$ at 2 kHz	93	dB	
		ADS8471IB		93		
		ADS8471I	$V_{IN} = 4 V_{pp}$ at 20 kHz	92.4		
		ADS8471IB		92.6		
		ADS8471I	$V_{IN} = 4 V_{pp}$ at 100 kHz	91		
		ADS8471IB		91.1		
SFDR	Spurious free dynamic range ⁽¹⁾	ADS8471I	$V_{IN} = 4 V_{pp}$ at 2 kHz	112	dB	
		ADS8471IB		114		
		ADS8471I	$V_{IN} = 4 V_{pp}$ at 20 kHz	107		
		ADS8471IB		109		
		ADS8471I	$V_{IN} = 4 V_{pp}$ at 100 kHz	102		
		ADS8471IB		103		
-3dB Small signal bandwidth				15		MHz
VOLTAGE REFERENCE INPUT						
V_{ref}	Reference voltage at REFIN,		3.0	4.096	+VA - 0.8	V
	Reference resistance ⁽²⁾			500		k Ω
	Reference current drain	$f_s = 1\text{ MHz}$			1	mA

(1) Calculated on the first nine harmonics of the input frequency.

(2) Can vary $\pm 20\%$

SPECIFICATIONS (Continued)
 $T_A = -40\text{C}$ to 85C , $+VA = 5\text{ V}$, $+VBD = 3\text{ V}$ or 5 V , $V_{ref} = 4.096\text{ V}$, $f_{SAMPLE} = 1\text{ MSPS}$ (unless otherwise noted)

PARAMETER		TEST CONDITIONS	MIN	TYP	MAX	UNIT
INTERNAL REFERENCE OUTPUT						
Internal reference start-up time		From 95% (+VA), with 1- μF storage capacitor			120	ms
V_{ref}	Reference voltage range	$I_O = 0\text{ A}$	4.081	4.096	4.111	V
Source current		Static load			10	μA
Line regulation		$+VA = 4.75\text{ V}$ to 5.25 V		60		μV
Drift		$I_O = 0\text{ A}$		± 6		PPM/ $^{\circ}\text{C}$
DIGITAL INPUT/OUTPUT						
Logic family – CMOS						
V_{IH}	High-level input voltage	$I_{IH} = 5\text{ }\mu\text{A}$	$+VBD - 1$		$+VBD + 0.3$	V
V_{IL}	Low-level input voltage	$I_{IL} = 5\text{ }\mu\text{A}$	-0.3		0.8	
V_{OH}	High-level output voltage	$I_{OH} = 2\text{ TTL loads}$	$+VBD - 0.6$			
V_{OL}	Low-level output voltage	$I_{OL} = 2\text{ TTL loads}$			0.4	
Data format – Straight binary						
POWER SUPPLY REQUIREMENTS						
Power supply voltage	+VBD		2.7	3.3	5.25	V
	+VA		4.75	5	5.25	V
Supply current ⁽¹⁾		$f_s = 1\text{ MHz}$		44	48	mA
Power dissipation ⁽¹⁾		$f_s = 1\text{ MHz}$		220	240	mW
TEMPERATURE RANGE						
Operating free-air			-40		85	$^{\circ}\text{C}$

(1) This includes only +VA current. +VBD current is typical 1 mA with 5-pF load capacitance on all output pins.

TIMING CHARACTERISTICS

All specifications typical at -40°C to 85°C , $+V_A = +V_{BD} = 5\text{ V}$ ⁽¹⁾ ⁽²⁾ ⁽³⁾

PARAMETER		MIN	TYP	MAX	UNIT
$t_{(\text{CONV})}$	Conversion time		670	700	ns
$t_{(\text{ACQ})}$	Acquisition time	270	300		ns
$t_{(\text{HOLD})}$	Sample capacitor hold time			25	ns
t_{pd1}	$\overline{\text{CONVST}}$ low to BUSY high			40	ns
t_{pd2}	Propagation delay time, end of conversion to BUSY low			15	ns
t_{pd3}	Propagation delay time, start of convert state to rising edge of BUSY			15	ns
t_{w1}	Pulse duration, $\overline{\text{CONVST}}$ low	40			ns
t_{su1}	Setup time, $\overline{\text{CS}}$ low to $\overline{\text{CONVST}}$ low	20			ns
t_{w2}	Pulse duration, $\overline{\text{CONVST}}$ high	20			ns
	$\overline{\text{CONVST}}$ falling edge jitter			10	ps
t_{w3}	Pulse duration, BUSY signal low	$t_{(\text{ACQ})\text{min}}$			ns
t_{w4}	Pulse duration, BUSY signal high			700	ns
t_{h1}	Hold time, first data bus transition ($\overline{\text{RD}}$ low, or $\overline{\text{CS}}$ low for read cycle, or BYTE input changes) after $\overline{\text{CONVST}}$ low	40			ns
t_{d1}	Delay time, $\overline{\text{CS}}$ low to $\overline{\text{RD}}$ low	0			ns
t_{su2}	Setup time, $\overline{\text{RD}}$ high to $\overline{\text{CS}}$ high	0			ns
t_{w5}	Pulse duration, $\overline{\text{RD}}$ low	50			ns
t_{en}	Enable time, $\overline{\text{RD}}$ low (or $\overline{\text{CS}}$ low for read cycle) to data valid			20	ns
t_{d2}	Delay time, data hold from $\overline{\text{RD}}$ high	5			ns
t_{d3}	Delay time, BYTE rising edge or falling edge to data valid	10		20	ns
t_{w6}	Pulse duration, $\overline{\text{RD}}$ high	20			ns
t_{w7}	Pulse duration, $\overline{\text{CS}}$ high	20			ns
t_{h2}	Hold time, last $\overline{\text{RD}}$ (or $\overline{\text{CS}}$ for read cycle) rising edge to $\overline{\text{CONVST}}$ falling edge	50			ns
t_{pd4}	Propagation delay time, BUSY falling edge to next $\overline{\text{RD}}$ (or $\overline{\text{CS}}$ for read cycle) falling edge	0			ns
t_{d4}	Delay time, BYTE edge to edge skew	0			ns
t_{su3}	Setup time, BYTE transition to $\overline{\text{RD}}$ falling edge	10			ns
t_{h3}	Hold time, BYTE transition to $\overline{\text{RD}}$ falling edge	10			ns
t_{dis}	Disable time, $\overline{\text{RD}}$ high ($\overline{\text{CS}}$ high for read cycle) to 3-stated data bus			20	ns
t_{d5}	Delay time, BUSY low to MSB data valid delay			0	ns
t_{d6}	Delay time, $\overline{\text{CS}}$ rising edge to BUSY falling edge	50			ns
t_{d7}	Delay time, BUSY falling edge to $\overline{\text{CS}}$ rising edge	50			ns
t_{su5}	BYTE transition setup time, from BYTE transition to next BYTE transition	50			ns
$t_{\text{su}(\text{ABORT})}$	Setup time from the falling edge of $\overline{\text{CONVST}}$ (used to start the valid conversion) to the next falling edge of $\overline{\text{CONVST}}$ (when $\overline{\text{CS}} = 0$ and $\overline{\text{CONVST}}$ are used to abort) or to the next falling edge of $\overline{\text{CS}}$ (when $\overline{\text{CS}}$ is used to abort).	60		600	ns

(1) All input signals are specified with $t_r = t_f = 5\text{ ns}$ (10% to 90% of $+V_{BD}$) and timed from a voltage level of $(V_{IL} + V_{IH})/2$.

(2) See timing diagrams.

(3) All timing are measured with 20-pF equivalent loads on all data bits and BUSY pins.

TIMING CHARACTERISTICS

All specifications typical at -40°C to 85°C , $+V_A = 5\text{ V}$ $+V_{BD} = 3\text{ V}$ ⁽¹⁾ ⁽²⁾ ⁽³⁾

PARAMETER		MIN	TYP	MAX	UNIT
$t_{(\text{CONV})}$	Conversion time		67	700	ns
$t_{(\text{ACQ})}$	Acquisition time	270	300		ns
$t_{(\text{HOLD})}$	Sample capacitor hold time			25	ns
t_{pd1}	$\overline{\text{CONVST}}$ low to BUSY high			40	ns
t_{pd2}	Propagation delay time, end of conversion to BUSY low			25	ns
t_{pd3}	Propagation delay time, start of convert state to rising edge of BUSY			25	ns
t_{w1}	Pulse duration, $\overline{\text{CONVST}}$ low	40			ns
t_{su1}	Setup time, $\overline{\text{CS}}$ low to $\overline{\text{CONVST}}$ low	20			ns
t_{w2}	Pulse duration, CONVST high	20			ns
	$\overline{\text{CONVST}}$ falling edge jitter			10	ps
t_{w3}	Pulse duration, BUSY signal low	$t_{(\text{ACQ})\text{min}}$			ns
t_{w4}	Pulse duration, BUSY signal high			700	ns
t_{h1}	Hold time, first data bus transition ($\overline{\text{RD}}$ low, or $\overline{\text{CS}}$ low for read cycle, or BYTE input changes) after $\overline{\text{CONVST}}$ low	40			ns
t_{d1}	Delay time, $\overline{\text{CS}}$ low to $\overline{\text{RD}}$ low	0			ns
t_{su2}	Setup time, $\overline{\text{RD}}$ high to $\overline{\text{CS}}$ high	0			ns
t_{w5}	Pulse duration, $\overline{\text{RD}}$ low	50			ns
t_{en}	Enable time, $\overline{\text{RD}}$ low (or $\overline{\text{CS}}$ low for read cycle) to data valid			30	ns
t_{d2}	Delay time, data hold from $\overline{\text{RD}}$ high	5			ns
t_{d3}	Delay time, BYTE rising edge or falling edge to data valid	10		30	ns
t_{w6}	Pulse duration, $\overline{\text{RD}}$ high	20			ns
t_{w7}	Pulse duration, $\overline{\text{CS}}$ high	20			ns
t_{h2}	Hold time, last $\overline{\text{RD}}$ (or $\overline{\text{CS}}$ for read cycle) rising edge to $\overline{\text{CONVST}}$ falling edge	50			ns
t_{pd4}	Propagation delay time, BUSY falling edge to next $\overline{\text{RD}}$ (or $\overline{\text{CS}}$ for read cycle) falling edge	0			ns
t_{d4}	Delay time, BYTE edge to edge skew	0			ns
t_{su3}	Setup time, BYTE or transition to $\overline{\text{RD}}$ falling edge	10			ns
t_{h3}	Hold time, BYTE or transition to $\overline{\text{RD}}$ falling edge	10			ns
t_{dis}	Disable time, $\overline{\text{RD}}$ high ($\overline{\text{CS}}$ high for read cycle) to 3-stated data bus			30	ns
t_{d5}	Delay time, BUSY low to MSB data valid delay			0	ns
t_{d6}	Delay time, $\overline{\text{CS}}$ rising edge to BUSY falling edge	50			ns
t_{d7}	Delay time, BUSY falling edge to $\overline{\text{CS}}$ rising edge	50			ns
t_{su5}	BYTE transition setup time, from BYTE transition to next BYTE transition	50			ns
$t_{\text{su}(\text{ABORT})}$	Setup time from the falling edge of $\overline{\text{CONVST}}$ (used to start the valid conversion) to the next falling edge of $\overline{\text{CONVST}}$ (when $\text{CS} = 0$ and $\overline{\text{CONVST}}$ are used to abort) or to the next falling edge of $\overline{\text{CS}}$ (when $\overline{\text{CS}}$ is used to abort).	60		600	ns

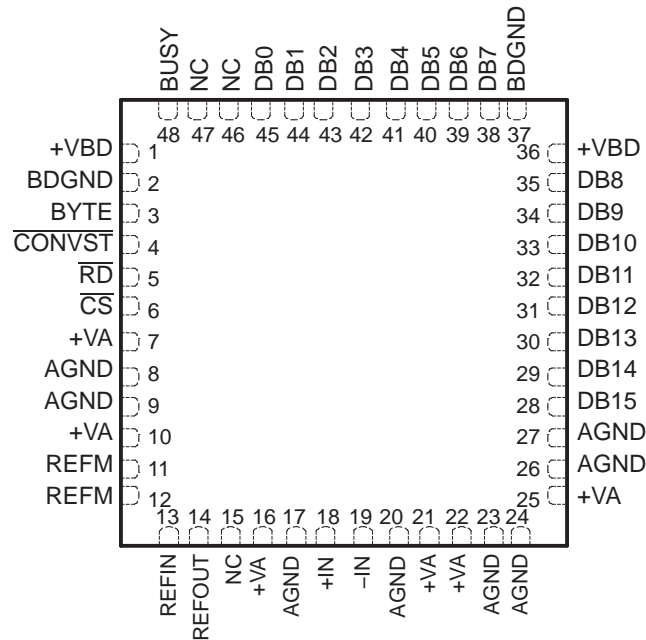
(1) All input signals are specified with $t_r = t_f = 5\text{ ns}$ (10% to 90% of $+V_{BD}$) and timed from a voltage level of $(V_{IL} + V_{IH})/2$.

(2) See timing diagrams.

(3) All timing are measured with 20-pF equivalent loads on all data bits and BUSY pins.

PIN ASSIGNMENTS

RGZ PACKAGE (TOP VIEW)



NC – No internal connection

NOTE: The package thermal pad must be soldered to the printed circuit board for thermal and mechanical performance.

TERMINAL FUNCTIONS

NAME	NO	I/O	DESCRIPTION		
AGND	8, 9, 17, 20, 23, 24, 26, 27	–	Analog ground		
BDGND	2, 37	–	Digital ground for bus interface digital supply		
BUSY	48	O	Status output. High when a conversion is in progress.		
BYTE	3	I	Byte select input. Used for 8-bit bus reading. 0: No fold back 1: Low byte D[9:2] of the 16 most significant bits is folded back to high byte of the 16 most significant pins DB[17:10].		
CONVST	4	I	Convert start. The falling edge of this input ends the acquisition period and starts the hold period.		
CS	6	I	Chip select. The falling edge of this input starts the acquisition period.		
Data Bus			8-BIT BUS		16-BIT BUS
			BYTE = 0	BYTE = 1	BYTE = 0
DB15	28	O	D15 (MSB)	D7	D15(MSB)
DB14	29	O	D14	D6	D14
DB13	30	O	D13	D5	D13
DB12	31	O	D12	D4	D12
DB11	32	O	D11	D3	D11
DB10	33	O	D10	D2	D10
DB9	34	O	D9	All ones	D9
DB8	35	O	D8	All ones	D8
DB7	38	O	D7	All ones	D7
DB6	39	O	D6	All ones	D6
DB5	40	O	D5	All ones	D5
DB4	41	O	D4	All ones	D4
DB3	42	O	D3	All ones	D3

TERMINAL FUNCTIONS (continued)

NAME	NO	I/O	DESCRIPTION		
DB2	43	O	D2	All ones	D2
DB1	44	O	D1	All ones	D1
DB0	45	O	D0 (LSB)	All ones	D0 (LSB)
-IN	19	I	Inverting input channel		
+IN	18	I	Noninverting input channel		
NC	15, 46, 47		No connection		
REFIN	13	I	Reference input		
REFOUT	14	O	Reference output. Add 1- μ F capacitor between the REFOUT pin and REFM pin when internal reference is used.		
REFM	11, 12	I	Reference ground		
\overline{RD}	5	I	Synchronization pulse for the parallel output. When \overline{CS} is low, this serves as output enable and puts the previous conversion results on the bus.		
+VA	7, 10, 16, 21, 22, 25	-	Analog power supplies, 5-V DC		
+VBD	1, 36	-	Digital power supply for bus		

TYPICAL CHARACTERISTICS

DC HISTOGRAM
(8192 Conversion Outputs)

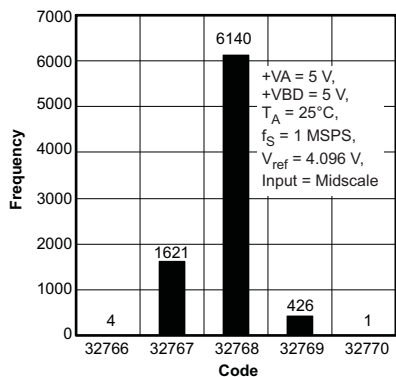


Figure 1.

INTERNAL REFERENCE VOLTAGE
vs
FREE-AIR TEMPERATURE

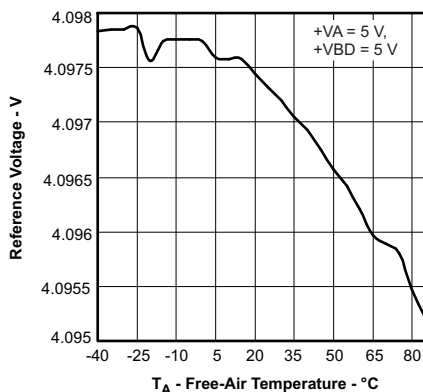


Figure 2.

INTERNAL REFERENCE VOLTAGE
vs
SUPPLY VOLTAGE

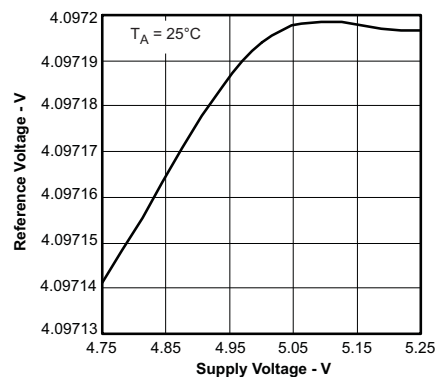


Figure 3.

SUPPLY CURRENT
vs
FREE-AIR TEMPERATURE

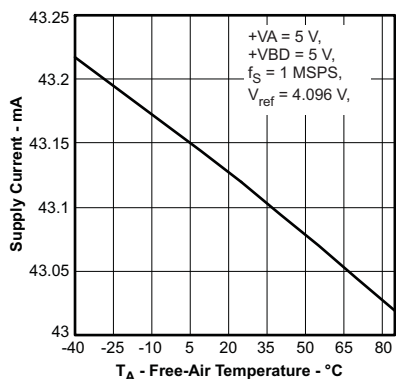


Figure 4.

SUPPLY CURRENT
vs
SUPPLY VOLTAGE

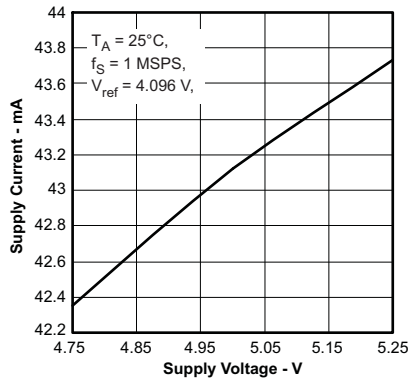


Figure 5.

SUPPLY CURRENT
vs
SAMPLE RATE

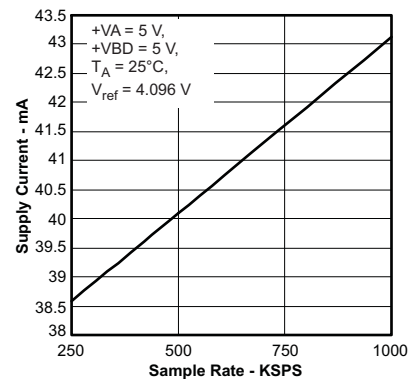


Figure 6.

TYPICAL CHARACTERISTICS (continued)

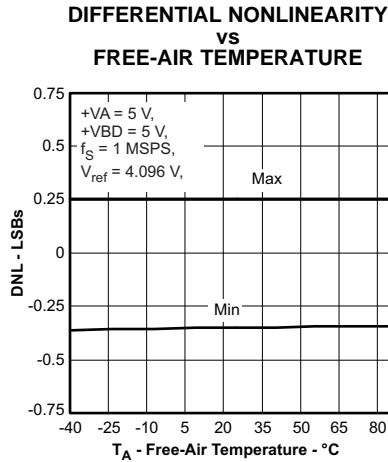


Figure 7.

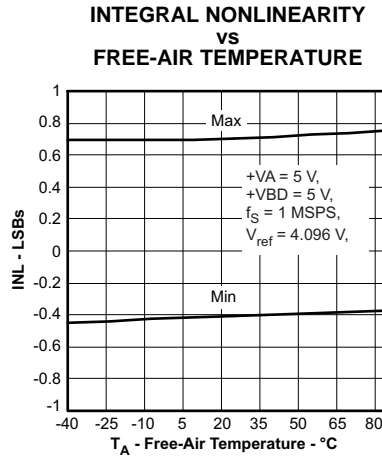


Figure 8.

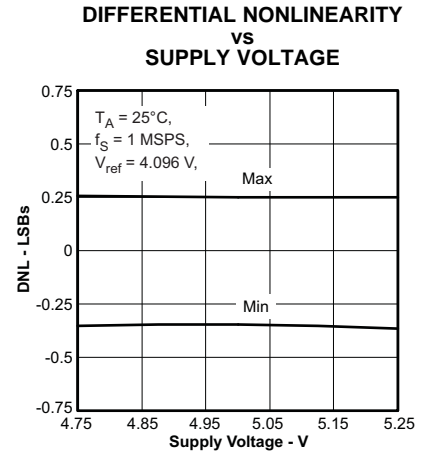


Figure 9.

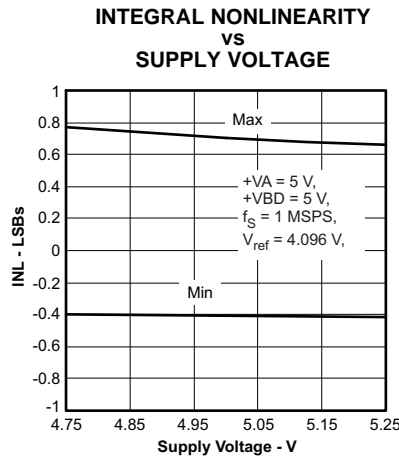


Figure 10.

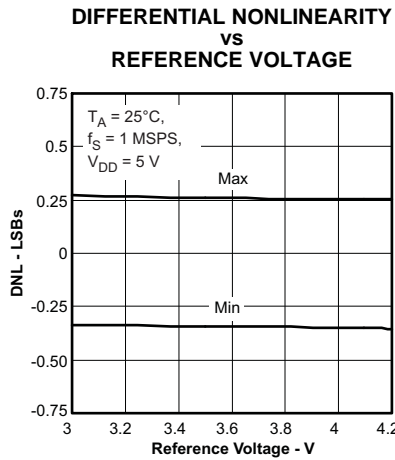


Figure 11.

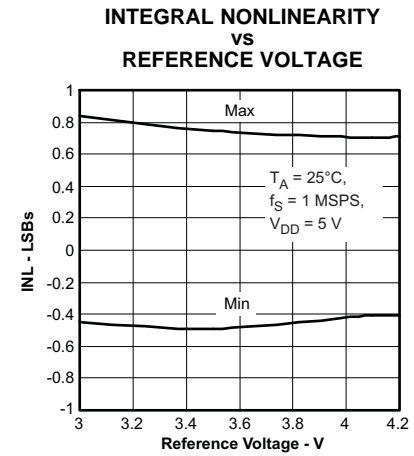


Figure 12.

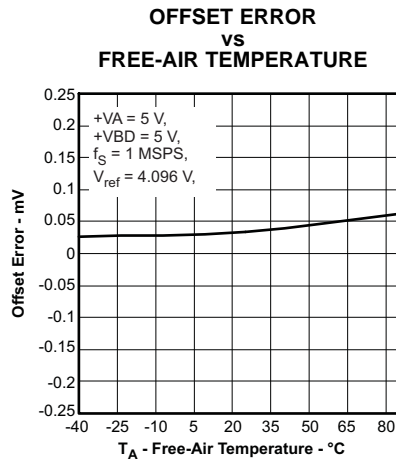


Figure 13.

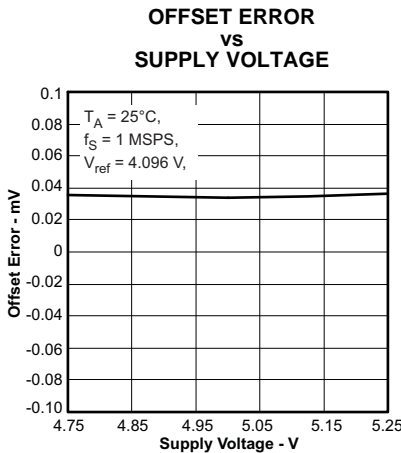


Figure 14.

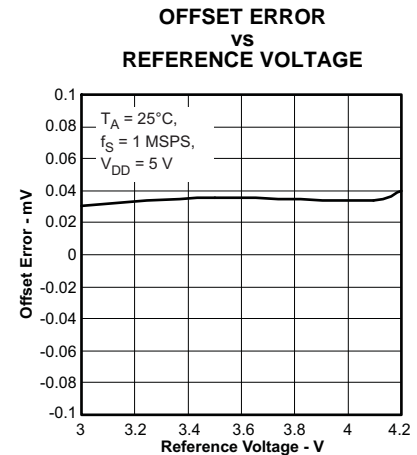


Figure 15.

TYPICAL CHARACTERISTICS (continued)

GAIN ERROR
vs
SUPPLY VOLTAGE

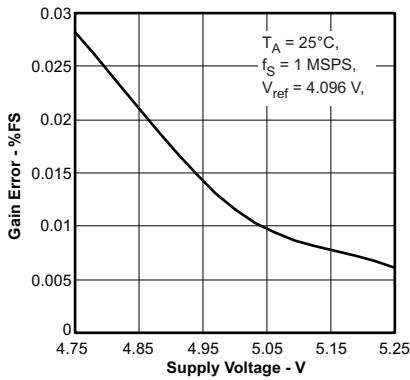


Figure 16.

GAIN ERROR
vs
FREE-AIR TEMPERATURE

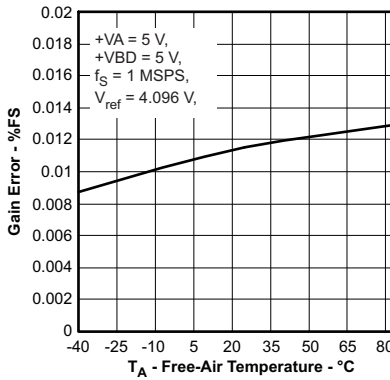


Figure 17.

GAIN ERROR
vs
REFERENCE VOLTAGE

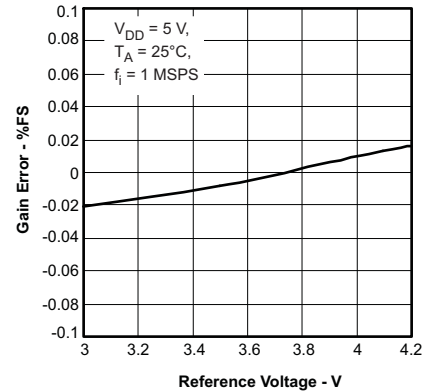


Figure 18.

OFFSET ERROR TEMPERATURE
DRIFT DISTRIBUTION (25 Samples)

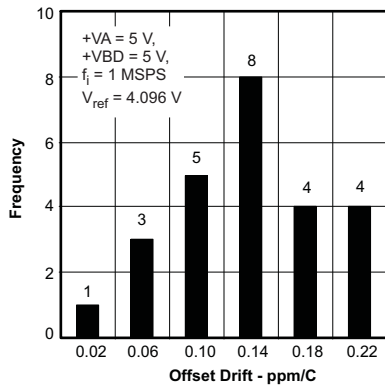


Figure 19.

GAIN ERROR TEMPERATURE
DRIFT DISTRIBUTION (25 Samples)

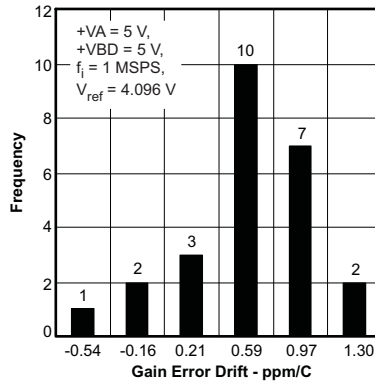


Figure 20.

TOTAL HARMONIC DISTORTION
vs
REFERENCE VOLTAGE

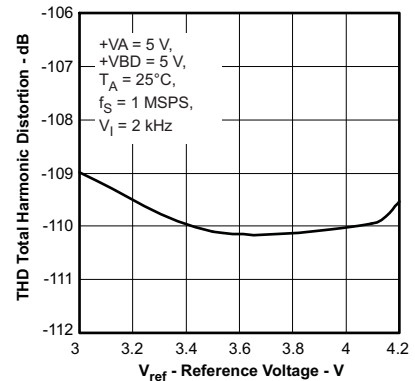


Figure 21.

SIGNAL-TO-NOISE RATIO
vs
REFERENCE VOLTAGE

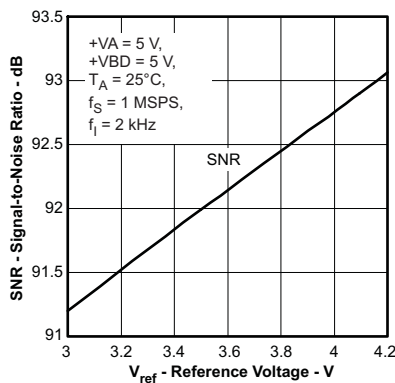


Figure 22.

SIGNAL-TO-NOISE + DISTORTION
vs
REFERENCE VOLTAGE

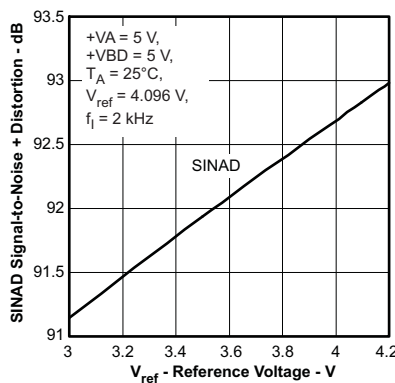


Figure 23.

TOTAL HARMONIC DISTORTION
vs
FREE-AIR TEMPERATURE

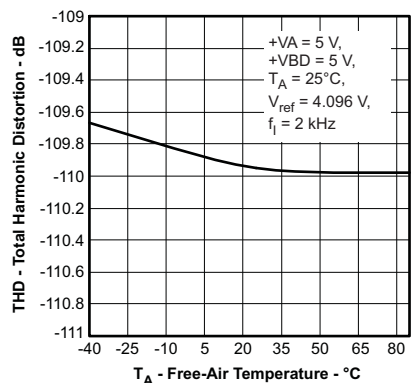


Figure 24.

TYPICAL CHARACTERISTICS (continued)

SPURIOUS FREE DYNAMIC RANGE
vs
FREE-AIR TEMPERATURE

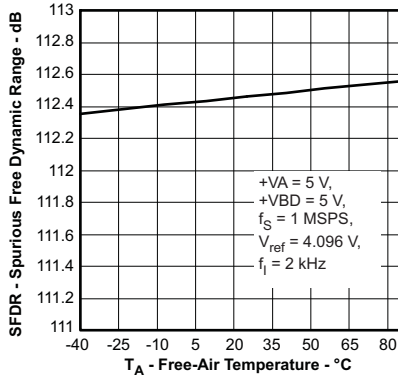


Figure 25.

SIGNAL-TO-NOISE RATIO
vs
FREE-AIR TEMPERATURE

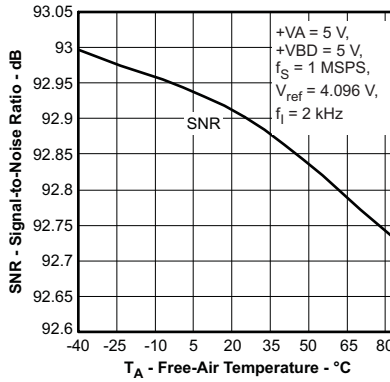


Figure 26.

SIGNAL-TO-NOISE + DISTORTION
vs
FREE-AIR TEMPERATURE

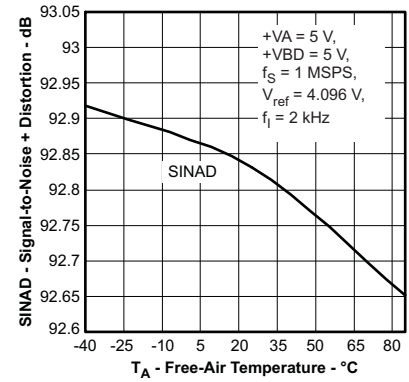


Figure 27.

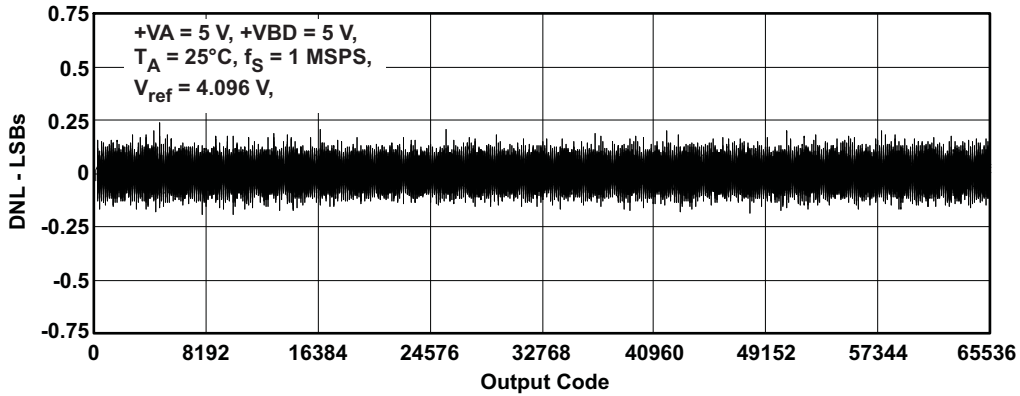


Figure 28.

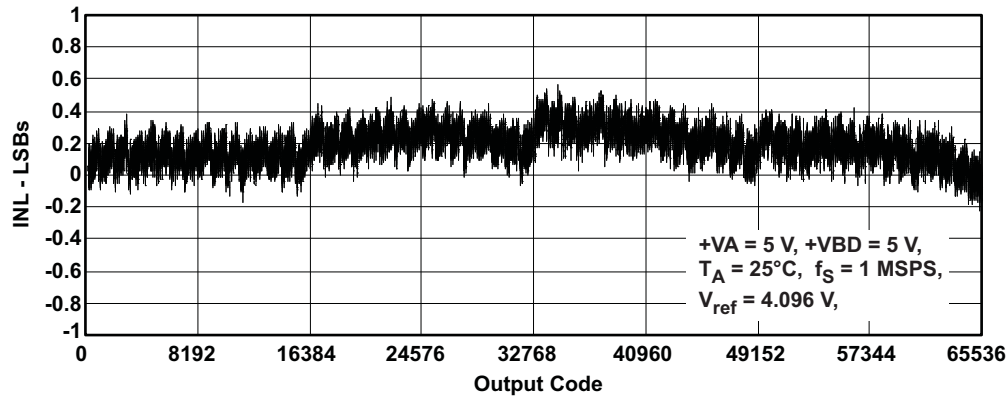


Figure 29.

TYPICAL CHARACTERISTICS (continued)

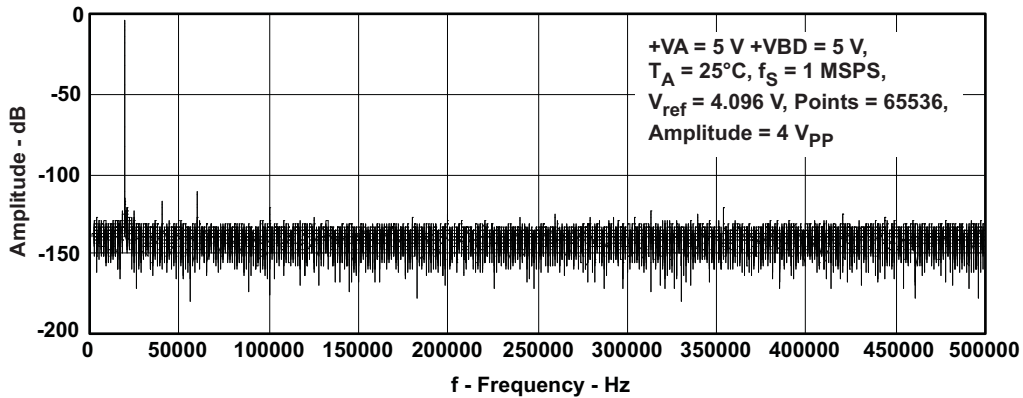


Figure 30.

TIMING DIAGRAMS

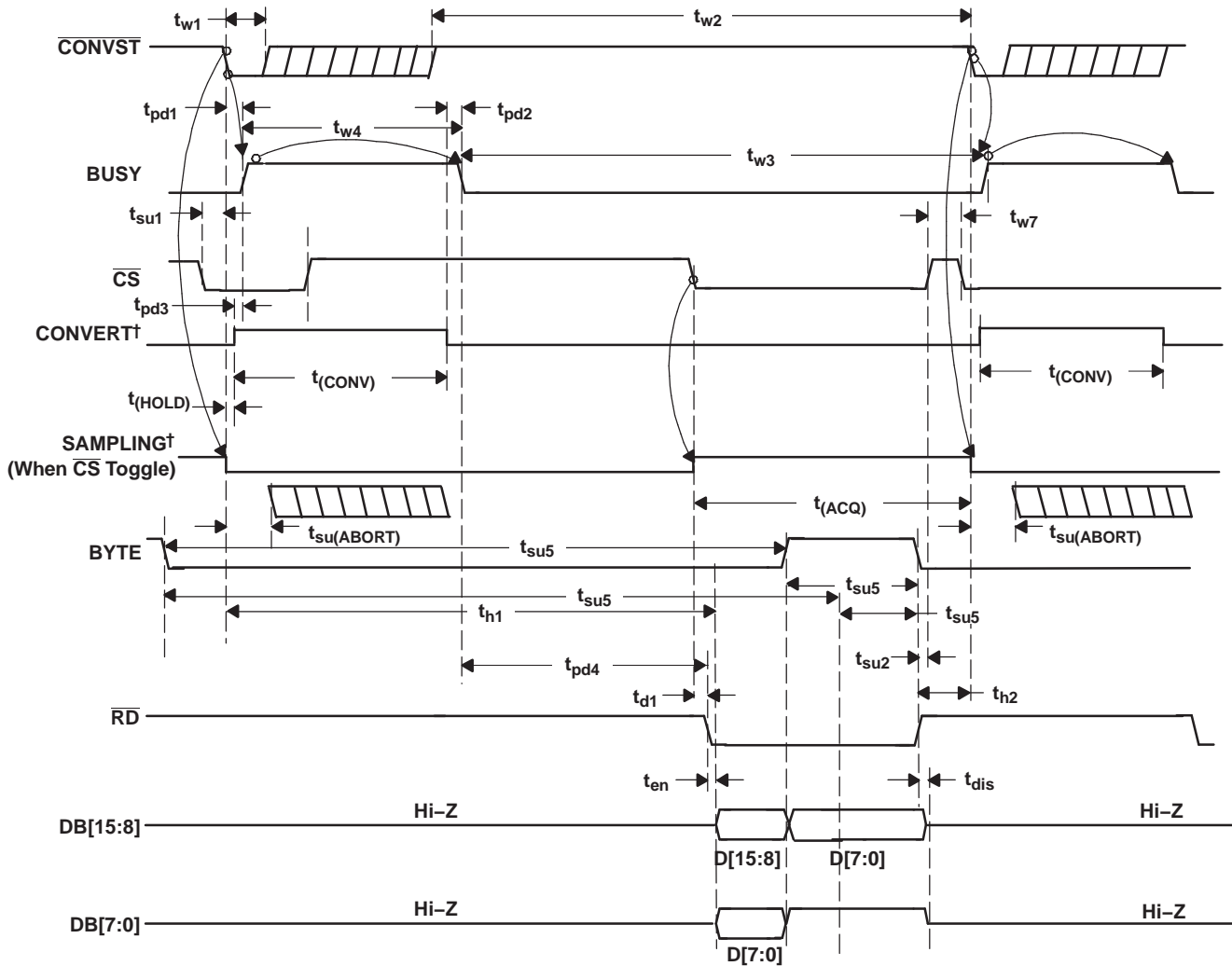
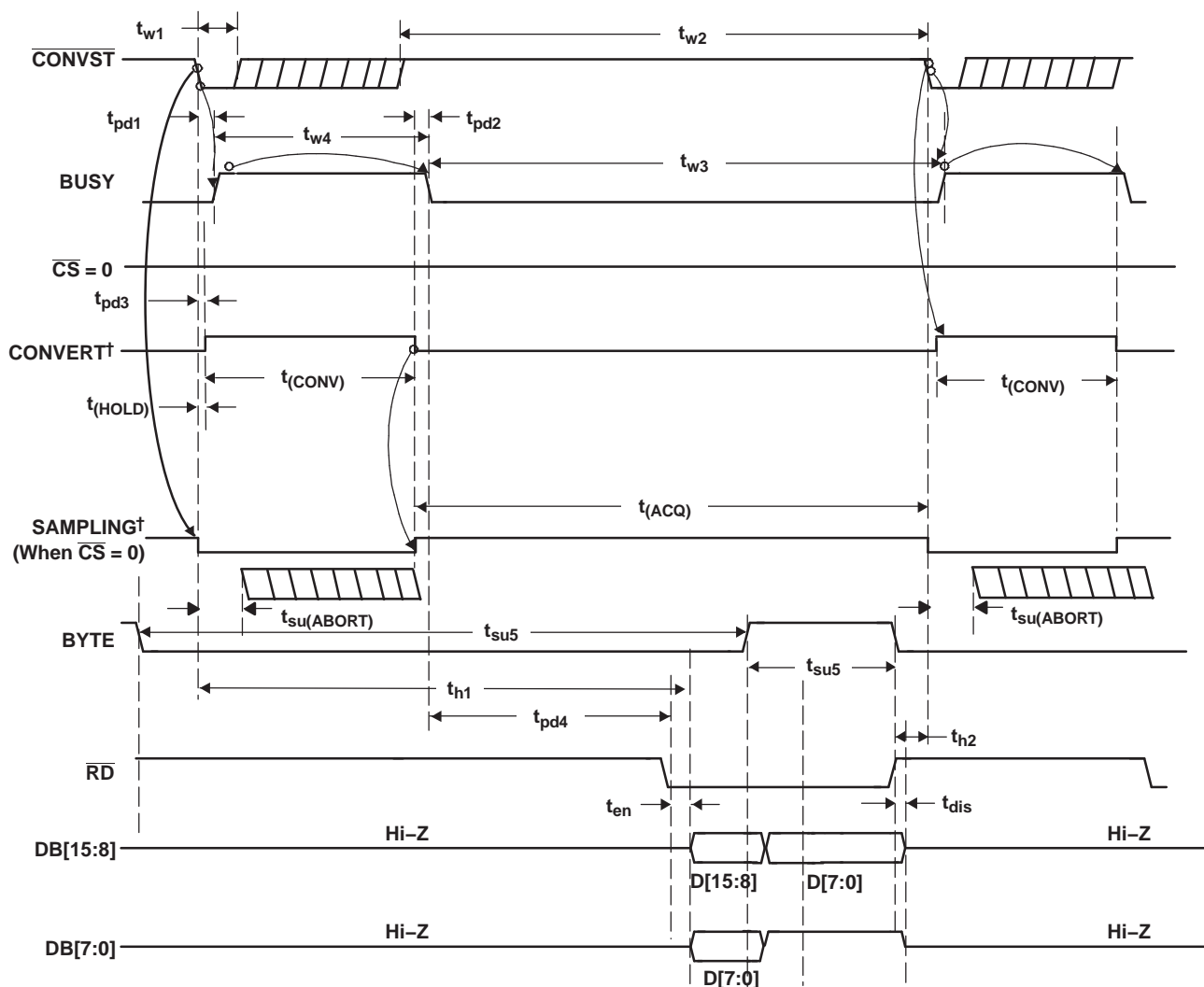


Figure 31. Timing for Conversion and Acquisition Cycles With \overline{CS} and \overline{RD} Toggling

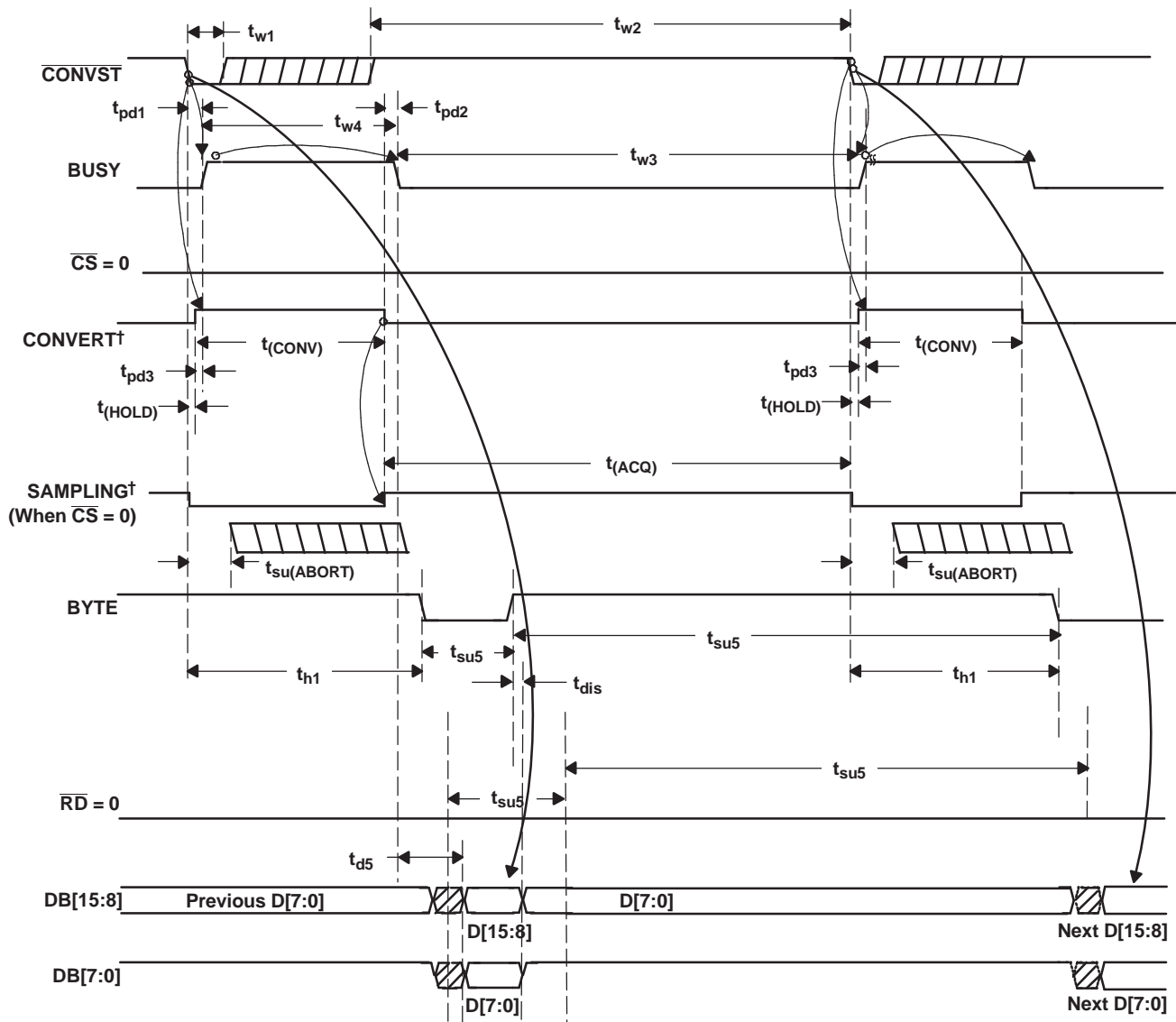
TYPICAL CHARACTERISTICS (continued)



†Signal internal to device

Figure 33. Timing for Conversion and Acquisition Cycles With \overline{CS} Tied to BDGND, \overline{RD} Toggling

TYPICAL CHARACTERISTICS (continued)



†Signal internal to device

Figure 34. Timing for Conversion and Acquisition Cycles With \overline{CS} and \overline{RD} Tied to BDGND - Auto Read

TYPICAL CHARACTERISTICS (continued)

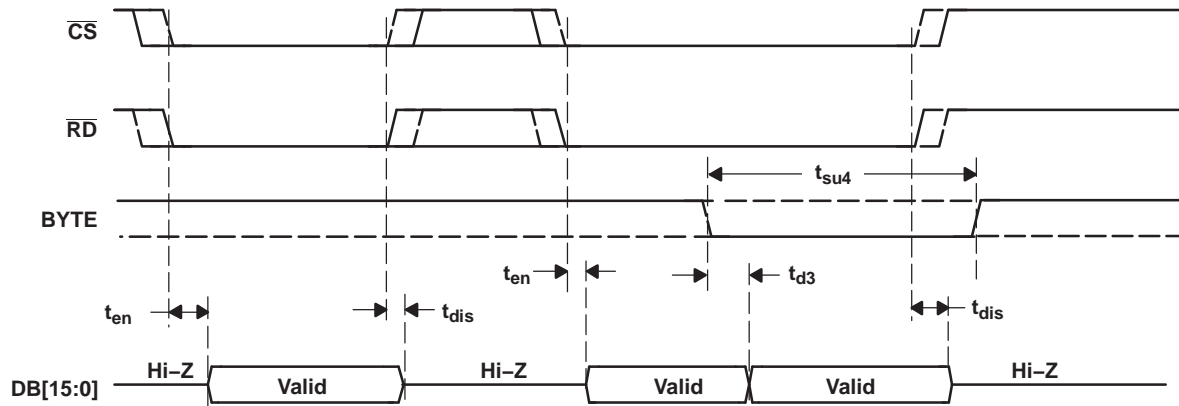


Figure 35. Detailed Timing for Read Cycles

APPLICATION INFORMATION

ADS8471 TO A HIGH PERFORMANCE DSP INTERFACE

Figure 36 shows a parallel interface between the ADS8471 and a Texas instruments high performance DSP such as the TMS320C6713 using the full 16-bit bus. The ADS8471 is mapped onto the $\overline{CE2}$ memory space of the TMS320C6713 DSP. The read and reset signals are generated by using a 3-to-8 decoder. A read operation from the address 0xA000C000 generates a pulse on the \overline{RD} pin of the data converter, whereas a read operation from word address 0xA0014000 generates a pulse on the $\overline{RESET/PD1}$ pin. The $\overline{CE2}$ signal of the DSP acts as \overline{CS} (chip select) for the converter. As the TMS320C6713 features a 32-bit external memory interface, the BYTE input of the converter can be tied permanently low, disabling the foldback of the data bus. The BUSY signal of the ADS8471 is applied to the $\overline{EXT_INT6}$ interrupt input of the DSP, enabling the EDMA controller to react on the falling edge of this signal and to collect the conversion result. The TOUT1 (timer out 1) pin of the TMS320C6713 is used to source the CONVST signal of the converter.

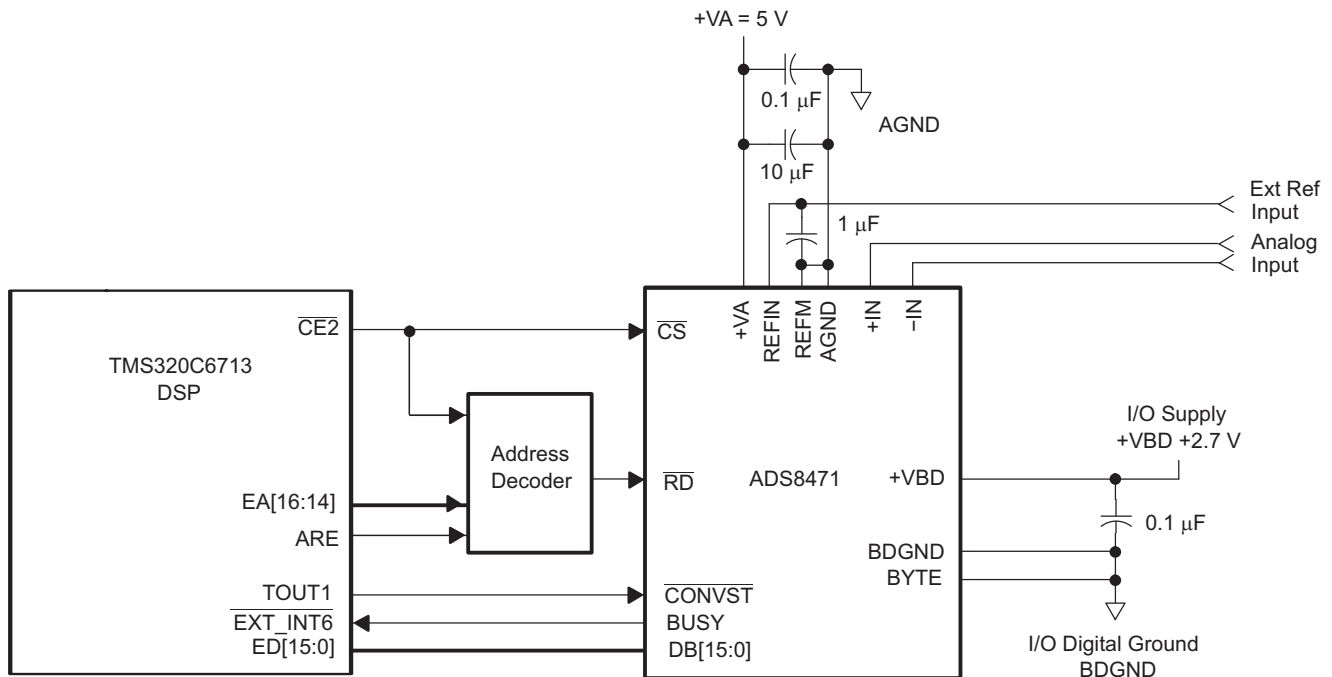


Figure 36. ADS8471 Application Circuitry

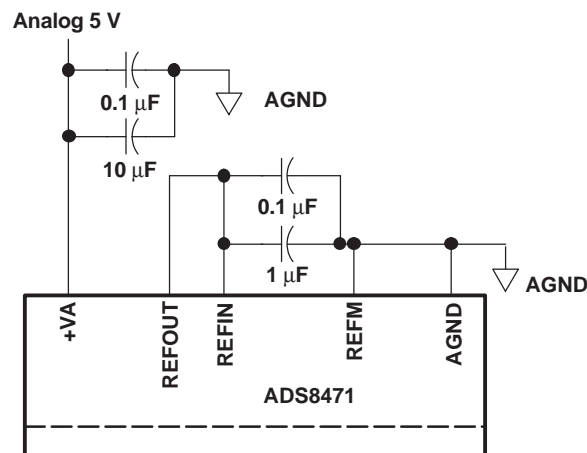


Figure 37. ADS8471 Using Internal Reference

PRINCIPLES OF OPERATION

The ADS8471 is a high-speed successive approximation register (SAR) analog-to-digital converter (ADC). The architecture is based on charge redistribution which inherently includes a sample/hold function. See [Figure 36](#) for the application circuit for the ADS8471.

The conversion clock is generated internally. The conversion time of 700 ns is capable of sustaining a 1-MHz throughput.

The analog input is provided to two input pins: +IN and –IN. When a conversion is initiated, the differential input on these pins is sampled on the internal capacitor array. While a conversion is in progress, both inputs are disconnected from any internal function.

REFERENCE

The ADS8471 can operate with an external reference with a range from 3.0 V to 4.2 V. The reference voltage on the input pin 13 (REFIN) of the converter is internally buffered. A clean, low noise, well-decoupled reference voltage on this pin is required to ensure good performance of the converter. A low noise band-gap reference like the REF5040 can be used to drive this pin. A 0.1- μ F decoupling capacitor is required between REFIN and REFM pins (pin 13 and pin 12) of the converter. This capacitor should be placed as close as possible to the pins of the device. Designers should strive to minimize the routing length of the traces that connect the terminals of the capacitor to the pins of the converter. An RC network can also be used to filter the reference voltage. A 100- Ω series resistor and a 0.1- μ F capacitor, which can also serve as the decoupling capacitor can be used to filter the reference voltage.

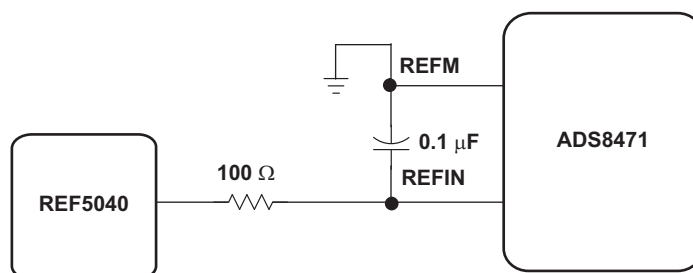


Figure 38. ADS8471 Using External Reference

The ADS8471 also has limited low pass filtering capability built into the converter. The equivalent circuitry on the REFIN input is as shown in [Figure 39](#).

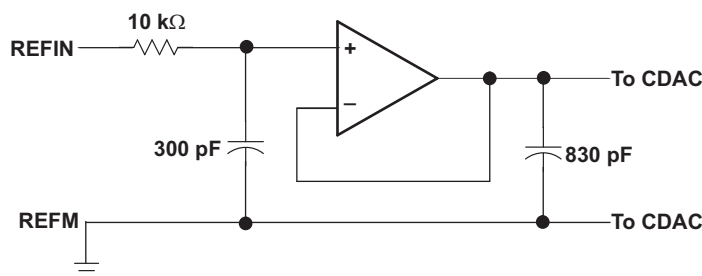


Figure 39. Reference Circuit

The REFM input of the ADS8471 should always be shorted to AGND.

A 4.096-V internal reference is included. When internal reference is used, pin 14 (REFOUT) is connected to pin 13 (REFIN) with a 0.1- μ F decoupling capacitor and 1- μ F storage capacitor between pin 14 (REFOUT) and pins 11 and 12 (REFM) (see [Figure 37](#)). The internal reference of the converter is double buffered. If an external reference is used, the second buffer provides isolation between the external reference and the CDAC. This buffer is also used to recharge all of the capacitors of the CDAC during conversion. Pin 14 (REFOUT) can be left unconnected (floating) if an external reference is used.

ANALOG INPUT

When the converter enters the hold mode, the voltage difference between the +IN and –IN inputs is captured on the internal capacitor array. The voltage on the –IN input is limited between -0.2 V and 0.2 V , allowing the input to reject small signals which are common to both the +IN and –IN inputs. The +IN input has a range of -0.2 V to $V_{\text{ref}} + 0.2\text{ V}$. The input span [+IN – (–IN)] is limited to 0 V to V_{ref} .

The input current on the analog inputs depends upon a number of factors: sample rate, input voltage, and source impedance. Essentially, the current into the ADS8471 charges the internal capacitor array during the sample period. After this capacitance has been fully charged, there is no further input current. The source of the analog input voltage must be able to charge the input capacitance (65 pF) to an 16-bit settling level within the acquisition time (270 ns) of the device. When the converter goes into the hold mode, the input impedance is greater than $1\text{ G}\Omega$.

Care must be taken regarding the absolute analog input voltage. To maintain the linearity of the converter, the +IN and –IN inputs and the span [+IN – (–IN)] must be within the limits specified. Outside of these ranges, the converter's linearity may not meet specifications. To minimize noise, low bandwidth input signals with low-pass filters are used.

Care must be taken to ensure that the output impedance of the sources driving the +IN and –IN inputs are matched. If this is not observed, the two inputs could have different settling times. This may result in offset error, gain error, and linearity error which varies with temperature and input voltage.

The analog input to the converter needs to be driven with a low noise, high-speed op-amp like the THS4031. An RC filter is recommended at the input pins to low-pass filter the noise from the source. A series resistor of $20\text{ }\Omega$ and a decoupling capacitor of 680 pF is recommended. The input to the converter is a uni-polar input voltage in the range 0 to V_{ref} . The THS4031 can be used in the source follower configuration to drive the converter (see [Figure 40](#)).

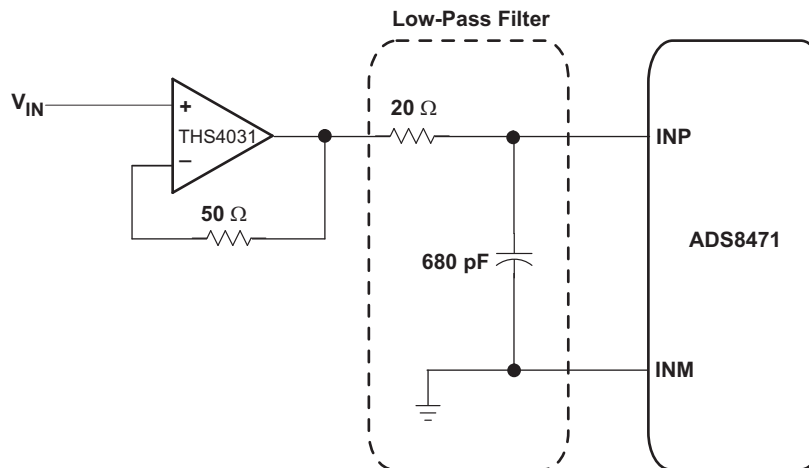


Figure 40. Unipolar Input Driving Circuit

In systems, where the input is bi-polar, the THS4031 can be used in the inverting configuration with an additional DC bias applied to its + input so as to keep the input to the ADS8471 within its rated operating voltage range (see [Figure 41](#)). This configuration is also recommended when the ADS8471 is used in signal processing applications where good SNR and THD performance is required. The DC bias can be derived from the REF3220 or the REF5040 reference voltage ICs. The input configuration shown below is capable of delivering better than 91dB SNR and -100db THD at an input frequency of 100 kHz. In case band-pass filters are used to filter the input, care should be taken to ensure that the signal swing at the input of the band-pass filter is small so as to keep the distortion introduced by the filter minimal. In such cases, the gain of the circuit shown below can be increased to keep the input to the ADS8471 large to keep the SNR of the system high. Note that the gain of the system from the + input to the output of the THS4031 in such a configuration is a function of the gain of the AC signal. A resistor divider can be used to scale the output of the REF3220 or REF5040 to reduce the voltage at the DC input to THS4031 to keep the voltage at the input of the converter within its rated operating range.

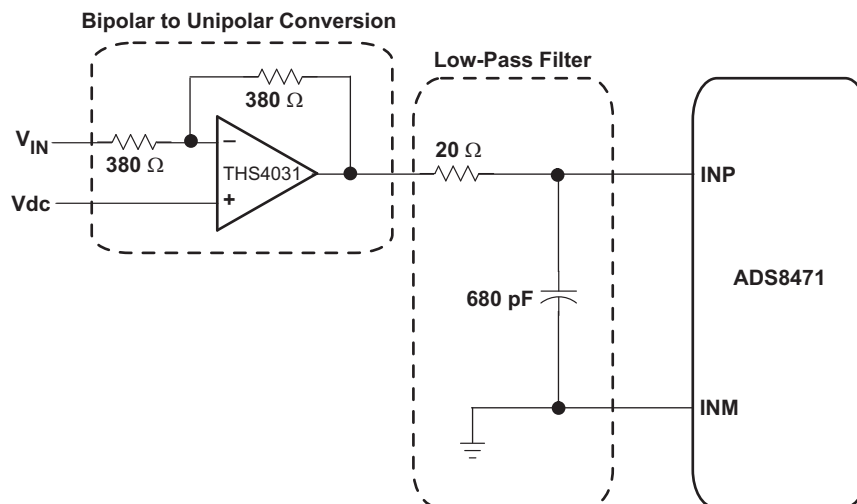


Figure 41. Bipolar Input Driving Circuit

DIGITAL INTERFACE

Timing and Control

See the timing diagrams in the specifications section for detailed information on timing signals and their requirements.

The ADS8471 uses an internal oscillator generated clock which controls the conversion rate and in turn the throughput of the converter. No external clock input is required.

Conversions are initiated by bringing the $\overline{\text{CONVST}}$ pin low for a minimum of 20 ns (after the 20 ns minimum requirement has been met, the $\overline{\text{CONVST}}$ pin can be brought high), while $\overline{\text{CS}}$ is low. The ADS8471 switches from the sample to the hold mode on the falling edge of the $\overline{\text{CONVST}}$ command. A clean and low jitter falling edge of this signal is important to the performance of the converter. The $\overline{\text{BUSY}}$ output is brought high immediately following $\overline{\text{CONVST}}$ going low. $\overline{\text{BUSY}}$ stays high throughout the conversion process and returns low when the conversion has ended.

Sampling starts with the falling edge of the $\overline{\text{BUSY}}$ signal when $\overline{\text{CS}}$ is tied low or starts with the falling edge of $\overline{\text{CS}}$ when $\overline{\text{BUSY}}$ is low.

Both $\overline{\text{RD}}$ and $\overline{\text{CS}}$ can be high during and before a conversion with one exception ($\overline{\text{CS}}$ must be low when $\overline{\text{CONVST}}$ goes low to initiate a conversion). Both the $\overline{\text{RD}}$ and $\overline{\text{CS}}$ pins are brought low in order to enable the parallel output bus with the conversion.

Reading Data

The ADS8471 outputs full parallel data in straight binary format as shown in Table 1. The parallel output is active when $\overline{\text{CS}}$ and $\overline{\text{RD}}$ are both low. There is a minimal quiet zone requirement around the falling edge of $\overline{\text{CONVST}}$. This is 50 ns prior to the falling edge of $\overline{\text{CONVST}}$ and 40 ns after the falling edge. No data read should be attempted within this zone. Any other combination of $\overline{\text{CS}}$ and $\overline{\text{RD}}$ sets the parallel output to 3-state. $\overline{\text{BYTE}}$ is used for multiword read operations. $\overline{\text{BYTE}}$ is used whenever lower bits on the bus are output on the higher byte of the bus. Refer to Table 1 for ideal output codes.

Table 1. Ideal Input Voltages and Output Codes

DESCRIPTION	ANALOG VALUE	DIGITAL OUTPUT STRAIGHT BINARY	
		BINARY CODE	HEX CODE
Full scale range	$+V_{ref}$		
Least significant bit (LSB)	$+V_{ref}/65536$		
+Full scale	$(+V_{ref}) - 1 \text{ LSB}$	1111 1111 1111 1111	FFFF
Midscale	$+V_{ref}/2$	1000 0000 0000 0000	8000
Midscale – 1 LSB	$+V_{ref}/2 - 1 \text{ LSB}$	0111 1111 1111 1111	7FFF
Zero	0 V	0000 0000 0000 0000	0000

The output data is a full 16-bit word (D15–D0) on DB15–DB0 pins (MSB–LSB) if BYTE is low.

The result may also be read on an 8-bit bus for convenience. This is done by using only pins DB15–DB8. In this case two reads are necessary: the first as before, leaving BYTE low and reading the 8 most significant bits on pins DB15–DB8, then bringing BYTE high. When BYTE is high, the low bits (D7–D0) appear on pins DB15–DB8.

All of these multiword read operations can be performed with multiple active \overline{RD} (toggling) or with \overline{RD} held low for simplicity. This is referred to as the AUTO READ operation.

Table 2. Conversion Data Read Out

BYTE	DATA READ OUT	
	PINS DB15–DB8	PINS DB7–DB0
High	D7-D0	All One's
Low	D15-D8	D7–D0

RESET

On power-up, internal POWER-ON RESET circuitry generates the reset required for the device. The first three conversions after power-up are used to load factory trimming data for a specific device to assure high accuracy of the converter. The results of the first three conversions are invalid and should be discarded.

The device can also be reset through the use of the combination of \overline{CS} and \overline{CONVST} . Since the BUSY signal is held at high during the conversion, either one of these conditions triggers an internal self-clear reset to the converter.

- Issue a \overline{CONVST} when \overline{CS} is low and the internal convert state is high. The falling edge of \overline{CONVST} starts a reset.
- Issue a \overline{CS} (select the device) while the internal convert state is high. The falling edge of \overline{CS} causes a reset.

Once the device is reset, all output latches are cleared (set to zeroes) and the BUSY signal is brought low. A new sampling period is started at the falling edge of the BUSY signal immediately after the instant of the internal reset.

LAYOUT

For optimum performance, care must be taken with the physical layout of the ADS8471 circuitry.

As the ADS8471 offers single-supply operation, it is often used in close proximity with digital logic, microcontrollers, microprocessors, and digital signal processors. The more digital logic present in the design and the higher the switching speed, the more difficult it is to achieve good performance from the converter.

The basic SAR architecture is sensitive to glitches or sudden changes on the power supply, reference, ground connections and digital inputs that occur just prior to latching the output of the analog comparator. Thus, driving any single conversion for an n-bit SAR converter, there are at least n windows in which large external transient voltages can affect the conversion result. Such glitches might originate from switching power supplies, nearby digital logic, or high power devices.

The degree of error in the digital output depends on the reference voltage, layout, and the exact timing of the external event.

On average, the ADS8471 draws very little current from an external reference as the reference voltage is internally buffered. If the reference voltage is external and originates from an op amp, make sure that it can drive the bypass capacitor or capacitors without oscillation. A 0.1- μ F capacitor is recommended from pin 13 (REFIN) directly to pin 12 (REFM). REFM and AGND must be shorted on the same ground plane under the device.






The AGND and BDGND pins should be connected to a clean ground point. In all cases, this should be the analog ground. Avoid connections which are too close to the grounding point of a microcontroller or digital signal processor. If required, run a ground trace directly from the converter to the power supply entry point. The ideal layout consists of an analog ground plane dedicated to the converter and associated analog circuitry.

As with the AGND connections, +VA should be connected to a 5-V power supply plane or trace that is separate from the connection for digital logic until they are connected at the power entry point. Power to the ADS8471 should be clean and well bypassed. A 0.1- μ F ceramic bypass capacitor should be placed as close to the device as possible. See [Table 3](#) for the placement of the capacitor. In addition, a 1- μ F to 10- μ F capacitor is recommended. In some situations, additional bypassing may be required, such as a 100- μ F electrolytic capacitor or even a Pi filter made up of inductors and capacitors—all designed to essentially low-pass filter the 5-V supply, removing the high frequency noise.

Table 3. Power Supply Decoupling Capacitor Placement

POWER SUPPLY PLANE	CONVERTER ANALOG SIDE	CONVERTER DIGITAL SIDE
SUPPLY PINS		
Pin pairs that require shortest path to decoupling capacitors	(7,8), (9,10), (16,17), (20,21), (22,23), (25,26)	36, 37
Pins that require no decoupling	24, 26	1,2

PACKAGING INFORMATION

Orderable Device	Status (1)	Package Type	Package Drawing	Pins	Package Qty	Eco Plan (2)	Lead/Ball Finish (6)	MSL Peak Temp (3)	Op Temp (°C)	Device Marking (4/5)	Samples
ADS8471IBRGZR	ACTIVE	VQFN	RGZ	48	2500	Green (RoHS & no Sb/Br)	CU NIPDAU	Level-2-260C-1 YEAR	-40 to 85	ADS 8471I B	
ADS8471IBRGZT	ACTIVE	VQFN	RGZ	48	250	Green (RoHS & no Sb/Br)	CU NIPDAU	Level-2-260C-1 YEAR	-40 to 85	ADS 8471I B	
ADS8471IRGZR	ACTIVE	VQFN	RGZ	48	2500	Green (RoHS & no Sb/Br)	CU NIPDAU	Level-2-260C-1 YEAR	-40 to 85	ADS 8471I	
ADS8471IRGZT	ACTIVE	VQFN	RGZ	48	250	Green (RoHS & no Sb/Br)	CU NIPDAU	Level-2-260C-1 YEAR	-40 to 85	ADS 8471I	
ADS8471IRGZTG4	ACTIVE	VQFN	RGZ	48	250	Green (RoHS & no Sb/Br)	CU NIPDAU	Level-2-260C-1 YEAR	-40 to 85	ADS 8471I	

(1) The marketing status values are defined as follows:

ACTIVE: Product device recommended for new designs.

LIFEBUY: TI has announced that the device will be discontinued, and a lifetime-buy period is in effect.

NRND: Not recommended for new designs. Device is in production to support existing customers, but TI does not recommend using this part in a new design.

PREVIEW: Device has been announced but is not in production. Samples may or may not be available.

OBSOLETE: TI has discontinued the production of the device.

(2) Eco Plan - The planned eco-friendly classification: Pb-Free (RoHS), Pb-Free (RoHS Exempt), or Green (RoHS & no Sb/Br) - please check <http://www.ti.com/productcontent> for the latest availability information and additional product content details.

TBD: The Pb-Free/Green conversion plan has not been defined.

Pb-Free (RoHS): TI's terms "Lead-Free" or "Pb-Free" mean semiconductor products that are compatible with the current RoHS requirements for all 6 substances, including the requirement that lead not exceed 0.1% by weight in homogeneous materials. Where designed to be soldered at high temperatures, TI Pb-Free products are suitable for use in specified lead-free processes.

Pb-Free (RoHS Exempt): This component has a RoHS exemption for either 1) lead-based flip-chip solder bumps used between the die and package, or 2) lead-based die adhesive used between the die and leadframe. The component is otherwise considered Pb-Free (RoHS compatible) as defined above.

Green (RoHS & no Sb/Br): TI defines "Green" to mean Pb-Free (RoHS compatible), and free of Bromine (Br) and Antimony (Sb) based flame retardants (Br or Sb do not exceed 0.1% by weight in homogeneous material)

(3) MSL, Peak Temp. - The Moisture Sensitivity Level rating according to the JEDEC industry standard classifications, and peak solder temperature.

(4) There may be additional marking, which relates to the logo, the lot trace code information, or the environmental category on the device.

(5) Multiple Device Markings will be inside parentheses. Only one Device Marking contained in parentheses and separated by a "~" will appear on a device. If a line is indented then it is a continuation of the previous line and the two combined represent the entire Device Marking for that device.

⁽⁶⁾ Lead/Ball Finish - Orderable Devices may have multiple material finish options. Finish options are separated by a vertical ruled line. Lead/Ball Finish values may wrap to two lines if the finish value exceeds the maximum column width.

Important Information and Disclaimer: The information provided on this page represents TI's knowledge and belief as of the date that it is provided. TI bases its knowledge and belief on information provided by third parties, and makes no representation or warranty as to the accuracy of such information. Efforts are underway to better integrate information from third parties. TI has taken and continues to take reasonable steps to provide representative and accurate information but may not have conducted destructive testing or chemical analysis on incoming materials and chemicals. TI and TI suppliers consider certain information to be proprietary, and thus CAS numbers and other limited information may not be available for release.

In no event shall TI's liability arising out of such information exceed the total purchase price of the TI part(s) at issue in this document sold by TI to Customer on an annual basis.

TAPE AND REEL INFORMATION

QUADRANT ASSIGNMENTS FOR PIN 1 ORIENTATION IN TAPE


*All dimensions are nominal

Device	Package Type	Package Drawing	Pins	SPQ	Reel Diameter (mm)	Reel Width W1 (mm)	A0 (mm)	B0 (mm)	K0 (mm)	P1 (mm)	W (mm)	Pin1 Quadrant
ADS8471IBRGZR	VQFN	RGZ	48	2500	330.0	16.4	7.3	7.3	1.5	12.0	16.0	Q2
ADS8471IBRGZT	VQFN	RGZ	48	250	180.0	16.4	7.3	7.3	1.5	12.0	16.0	Q2
ADS8471IRGZR	VQFN	RGZ	48	2500	330.0	16.4	7.3	7.3	1.5	12.0	16.0	Q2
ADS8471IRGZT	VQFN	RGZ	48	250	180.0	16.4	7.3	7.3	1.5	12.0	16.0	Q2

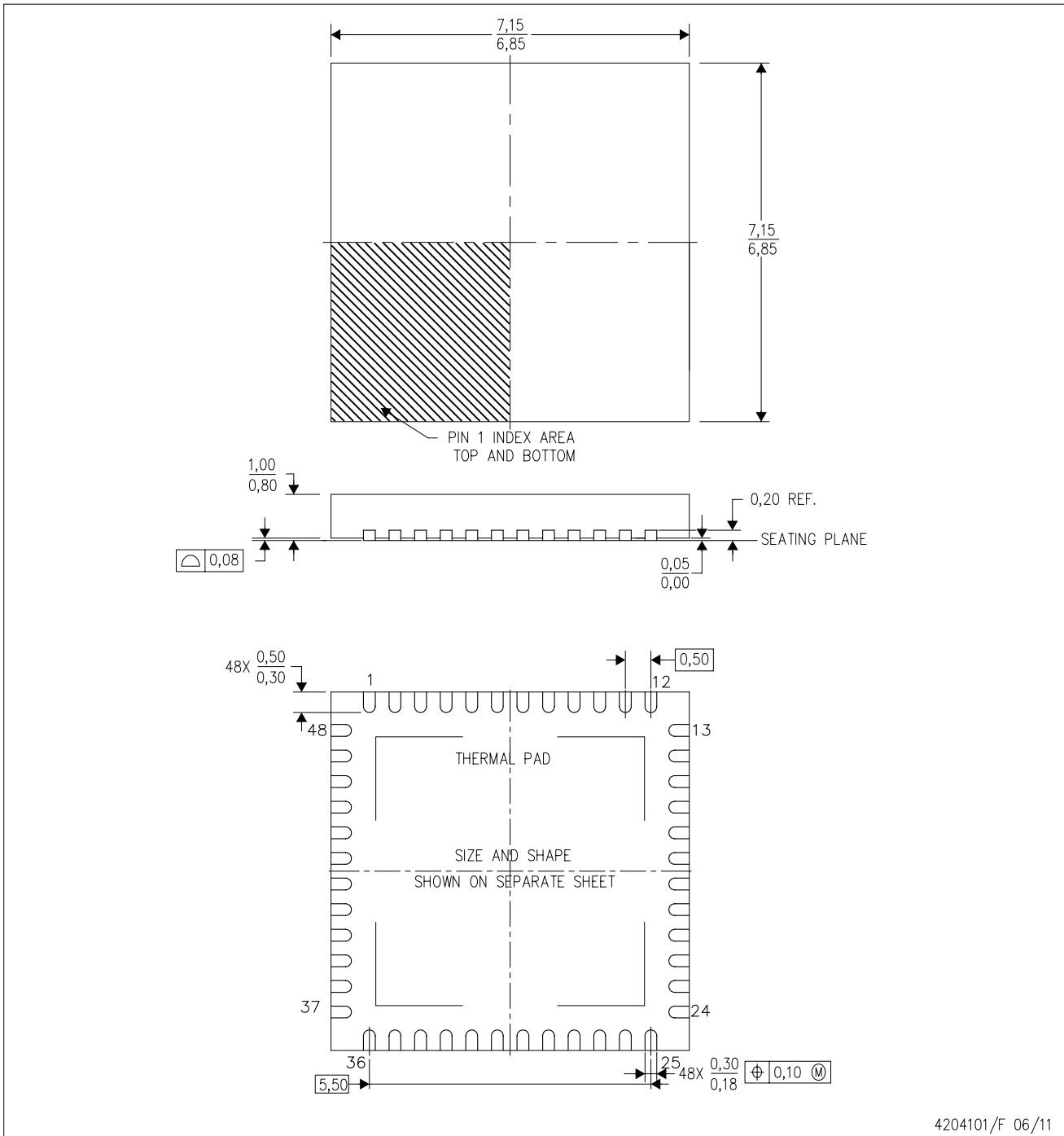
TAPE AND REEL BOX DIMENSIONS


*All dimensions are nominal

Device	Package Type	Package Drawing	Pins	SPQ	Length (mm)	Width (mm)	Height (mm)
ADS8471IBRGZR	VQFN	RGZ	48	2500	336.6	336.6	28.6
ADS8471IBRGZT	VQFN	RGZ	48	250	213.0	191.0	55.0
ADS8471IRGZR	VQFN	RGZ	48	2500	336.6	336.6	28.6
ADS8471IRGZT	VQFN	RGZ	48	250	213.0	191.0	55.0

RGZ (S-PVQFN-N48)

PLASTIC QUAD FLATPACK NO-LEAD



4204101/F 06/11

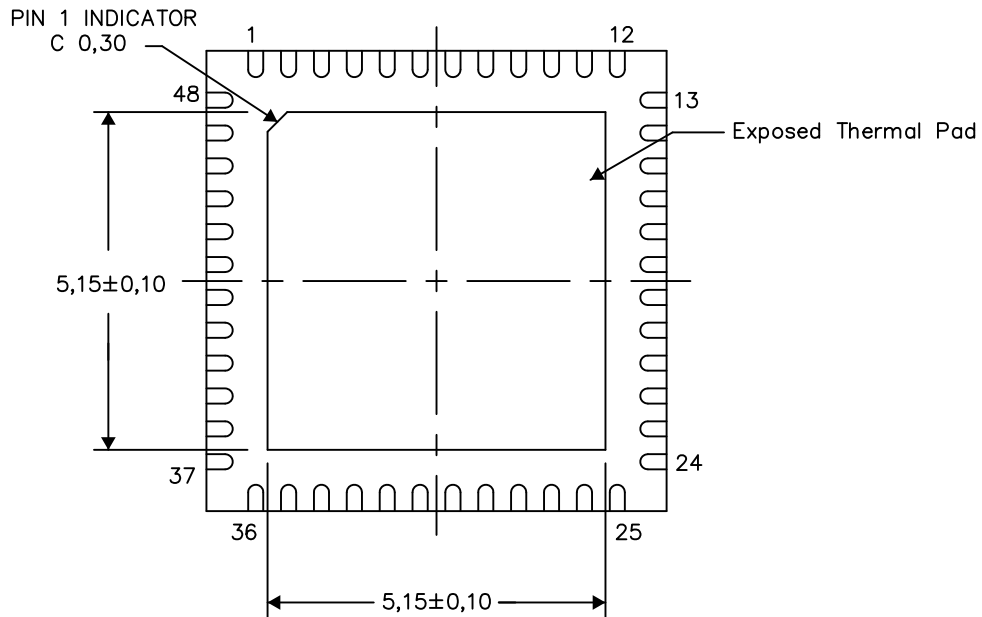
- NOTES:
- A. All linear dimensions are in millimeters. Dimensioning and tolerancing per ASME Y14.5M-1994.
 - B. This drawing is subject to change without notice.
 - C. Quad Flatpack, No-leads (QFN) package configuration.
 - D. The package thermal pad must be soldered to the board for thermal and mechanical performance.
 - E. See the additional figure in the Product Data Sheet for details regarding the exposed thermal pad features and dimensions.
 - F. Falls within JEDEC MO-220.

THERMAL INFORMATION

This package incorporates an exposed thermal pad that is designed to be attached directly to an external heatsink. The thermal pad must be soldered directly to the printed circuit board (PCB). After soldering, the PCB can be used as a heatsink. In addition, through the use of thermal vias, the thermal pad can be attached directly to the appropriate copper plane shown in the electrical schematic for the device, or alternatively, can be attached to a special heatsink structure designed into the PCB. This design optimizes the heat transfer from the integrated circuit (IC).

For information on the Quad Flatpack No-Lead (QFN) package and its advantages, refer to Application Report, QFN/SON PCB Attachment, Texas Instruments Literature No. SLUA271. This document is available at www.ti.com.

The exposed thermal pad dimensions for this package are shown in the following illustration.



Bottom View

Exposed Thermal Pad Dimensions

4206354-2/Y 06/14

NOTE: All linear dimensions are in millimeters

IMPORTANT NOTICE

Texas Instruments Incorporated and its subsidiaries (TI) reserve the right to make corrections, enhancements, improvements and other changes to its semiconductor products and services per JESD46, latest issue, and to discontinue any product or service per JESD48, latest issue. Buyers should obtain the latest relevant information before placing orders and should verify that such information is current and complete. All semiconductor products (also referred to herein as "components") are sold subject to TI's terms and conditions of sale supplied at the time of order acknowledgment.

TI warrants performance of its components to the specifications applicable at the time of sale, in accordance with the warranty in TI's terms and conditions of sale of semiconductor products. Testing and other quality control techniques are used to the extent TI deems necessary to support this warranty. Except where mandated by applicable law, testing of all parameters of each component is not necessarily performed.

TI assumes no liability for applications assistance or the design of Buyers' products. Buyers are responsible for their products and applications using TI components. To minimize the risks associated with Buyers' products and applications, Buyers should provide adequate design and operating safeguards.

TI does not warrant or represent that any license, either express or implied, is granted under any patent right, copyright, mask work right, or other intellectual property right relating to any combination, machine, or process in which TI components or services are used. Information published by TI regarding third-party products or services does not constitute a license to use such products or services or a warranty or endorsement thereof. Use of such information may require a license from a third party under the patents or other intellectual property of the third party, or a license from TI under the patents or other intellectual property of TI.

Reproduction of significant portions of TI information in TI data books or data sheets is permissible only if reproduction is without alteration and is accompanied by all associated warranties, conditions, limitations, and notices. TI is not responsible or liable for such altered documentation. Information of third parties may be subject to additional restrictions.

Resale of TI components or services with statements different from or beyond the parameters stated by TI for that component or service voids all express and any implied warranties for the associated TI component or service and is an unfair and deceptive business practice. TI is not responsible or liable for any such statements.

Buyer acknowledges and agrees that it is solely responsible for compliance with all legal, regulatory and safety-related requirements concerning its products, and any use of TI components in its applications, notwithstanding any applications-related information or support that may be provided by TI. Buyer represents and agrees that it has all the necessary expertise to create and implement safeguards which anticipate dangerous consequences of failures, monitor failures and their consequences, lessen the likelihood of failures that might cause harm and take appropriate remedial actions. Buyer will fully indemnify TI and its representatives against any damages arising out of the use of any TI components in safety-critical applications.

In some cases, TI components may be promoted specifically to facilitate safety-related applications. With such components, TI's goal is to help enable customers to design and create their own end-product solutions that meet applicable functional safety standards and requirements. Nonetheless, such components are subject to these terms.

No TI components are authorized for use in FDA Class III (or similar life-critical medical equipment) unless authorized officers of the parties have executed a special agreement specifically governing such use.

Only those TI components which TI has specifically designated as military grade or "enhanced plastic" are designed and intended for use in military/aerospace applications or environments. Buyer acknowledges and agrees that any military or aerospace use of TI components which have **not** been so designated is solely at the Buyer's risk, and that Buyer is solely responsible for compliance with all legal and regulatory requirements in connection with such use.

TI has specifically designated certain components as meeting ISO/TS16949 requirements, mainly for automotive use. In any case of use of non-designated products, TI will not be responsible for any failure to meet ISO/TS16949.

Products

Audio	www.ti.com/audio
Amplifiers	amplifier.ti.com
Data Converters	dataconverter.ti.com
DLP® Products	www.dlp.com
DSP	dsp.ti.com
Clocks and Timers	www.ti.com/clocks
Interface	interface.ti.com
Logic	logic.ti.com
Power Mgmt	power.ti.com
Microcontrollers	microcontroller.ti.com
RFID	www.ti-rfid.com
OMAP Applications Processors	www.ti.com/omap
Wireless Connectivity	www.ti.com/wirelessconnectivity

Applications

Automotive and Transportation	www.ti.com/automotive
Communications and Telecom	www.ti.com/communications
Computers and Peripherals	www.ti.com/computers
Consumer Electronics	www.ti.com/consumer-apps
Energy and Lighting	www.ti.com/energy
Industrial	www.ti.com/industrial
Medical	www.ti.com/medical
Security	www.ti.com/security
Space, Avionics and Defense	www.ti.com/space-avionics-defense
Video and Imaging	www.ti.com/video

TI E2E Community

e2e.ti.com